

RESEARCH PAPER

# Conformal antenna array for ultra-wideband direction-of-arrival estimation

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*The design and full-wave analysis of an antenna system for ultra-wideband radio direction finding applications is presented. The elliptical dipole antenna is selected as antenna element due to its robust circuital and radiation properties. The influence of the conformal deformation on the antenna performance has been studied in details. A suitable radome is designed to enhance the antenna front-to-back radiation ratio, as well as to increase the environmental durability of the structure. The considered antennas are optimized for their adoption in two different sub-arrays covering the [250, 950] MHz and [0.9, 3.3] GHz frequency bands, respectively. A uniform circular array (UCA) with five elements is used for the array topology. The full-wave analysis of the whole array structure is carried out in order to evaluate the coupling between the antenna elements. In particular, a novel calibration technique is developed in order to compensate for the mutual coupling between the array elements, possible variations in the antenna characteristics, and the effects of the array bearing structure. The performance of the designed array in terms of direction-of-arrival estimation is thoroughly analyzed and discussed.*

**Keywords:** Antenna design, Modeling and measurements, Radar applications, Radar signal processing and system Modeling

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## 1. INTRODUCTION

Due to its numerous applications, the problem of the direction-of-arrival (DOA) estimation of one or more incoming radio signals has attracted great attention in the industrial and scientific research communities. Radio direction finders (RDFs) have been widely employed in civil and military applications, e.g. for navigation [1]. In particular, the drastic increase of amount of different professional/commercial radio services operating over a very wide radio spectrum (from dozens of MHz to 6 GHz) triggered a demand for ultra-wideband (UWB) RDF systems covering the most popular part of the radio spectrum [2–7]. Existing RDF systems cannot however deal with these numerous applications due to their limited operational bandwidth. Thus, the design of UWB RDF systems is requested by different users. However, at the moment such designs are not investigated in open literature and are not commercially available.

RDF design is a cumbersome task that involves several disciplines such as antenna design, array calibration, signal processing algorithms for DOA estimation, and antenna array design. Ideally, UWB RDFs should feature a fractional bandwidth of at least 100% and small (in comparison to the largest wavelength) size, while still preserving an excellent performance in terms of DOA estimation accuracy. Since an RDF

usually utilizes circular or cylindrical arrays, compact and conformal antennas are needed to satisfy the requirements in terms of size, weight, and shape. In addition, the antenna elements should feature a large impedance bandwidth, a frequency-stable radiation pattern with a reasonable directivity level useful to improve the accuracy of the DOA estimation and reduce the probability of ambiguity, as well as demonstrate as low as possible parasitic coupling between the array elements and the support structure. For reliable performance of DOA estimation algorithms, the antenna elements must feature a stable phase center for different DOAs (although the negative effect of variations in the phase response can be mitigated with calibration, it is highly desirable to reduce the post processing). As RDFs generally track narrowband signals, the time-domain response of the antenna is not a critical parameter, although a large bandwidth is required. However, a low dispersion profile will be helpful when tracking UWB signals. Furthermore, suitable antenna covers are needed to increase the mechanical and environmental durability of the structure. However, since the cover has an important impact on the array performance, it must also be designed to enhance the antenna radiation properties.

Previous efforts on designing an antenna element dedicated to DOA estimation are mainly based on the adoption of dipoles and composite dipoles [8], log-periodic antennas [9], patch antenna arrays with electromagnetic band gap (EBG) substrates [10], and switched parasitic antennas [11–13].

As for the antenna array design, a uniform circular array (UCA) configuration is widely adopted in practice. Such configuration is preferable due to the complete radio coverage in the azimuthal angular direction [14]. In the determination of the number of array elements, the ambiguity issues are

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properly taken into account. An RDF is said to have a “rank- $n$ ” ambiguity if one steering vector is a linear combination of  $n$  other steering vectors [15]. Although the ambiguity problem still remains unsolved, some useful results about ambiguity issues in UCA are available in the scientific literature [14, 15].

To compensate the effects caused by parasitic coupling and variations in the antenna characteristics possibly responsible for a severe degradation of the system performance [16–18], suitable calibration methods can be adopted. Array calibration techniques may be classified into two different classes: deterministic and blind methods. Deterministic methods are off-line calibration techniques [19–22]. The antenna mutual coupling matrix is previously calculated, measured, or estimated and the errors are filtered out by means of a suitable matrix compensation. These techniques are very accurate and reliable, but have some disadvantages due to the fact that heavy numerical computation and accurate pattern measurements are required. However, the main drawback of such methods is that they cannot be used during the system operation. Hence, the effect of the environment is neglected. On the other hand, blind methods are on-line calibration techniques [23–25], based on the simultaneous estimation of the steering matrix and signal parameters. In general, there is no *a priori* assumption about the array topology or the antenna characteristics, so these methods are virtually immune to the effect of mutual coupling and errors. However, this can result in a waste of information potentially responsible for a poor resolution of the method, as well as a non-uniqueness of the solution.

The goal of this paper is to design a UWB RDF covering the band from 250 MHz to 3.3 GHz, where the accuracy of the estimation can vary depending on the application. Typical commercial systems feature a mean-square error (MSE) between 10 and 100 deg<sup>2</sup> [26]. The requirements considered in our design are to assure a probability of detection larger than 90% with a MSE smaller than 50 deg<sup>2</sup> over the whole operational bandwidth. A packet of radio signals is considered correctly detected when their exact number is determined and the MSE is smaller than 100 deg<sup>2</sup>. These requirements must be fulfilled when considering a maximum number of signals equals 3, a minimum separation between signals is equal to 10° and a minimum SNR of operation is equal to 8 dB. Since it is desirable to integrate RDF systems in mobile units, size constraints are usually provided. So, in order to make the antenna array suitable for a vehicle mounted system devoted to the control of the radio-frequency traffic, the maximum array radius is restricted to 45 cm for the low-frequency RDF subsystem, and to 13 cm for the high-frequency one. Furthermore, in order to avoid “rank-1” ambiguities in the estimation, the number of array elements must be either equal to 5, or equal or greater than 7 [14].

The design of such system has been carried out by using the following approach. Firstly, the individual antenna element is designed (Section II). The parasitic mutual coupling levels are evaluated by means of a full-wave analysis of the complete array structure, and a specially developed calibration technique is applied to compensate for both the mutual antenna coupling and the variations in the sensor characteristics (Section III). The performance evaluation of the designed RDF system is presented in Section IV. Section V summarizes the results and concludes this paper.

## II. SINGLE-ELEMENT ANTENNA DESIGN

We select an elliptically shaped dipole antenna [27–29] as an array element. Such antennas are inexpensive and readily manufacturable on conformal substrates to realize UCAs. They are characterized by relatively small volume occupation, the typical size being  $\lambda_0/5$  [27] at the lowest frequency of operation, where  $\lambda_0$  denotes the free space wavelength. In addition, these antennas are known to feature UWB behavior with a return loss level below  $-10$  dB over a fractional bandwidth of 10:1 or better [29]. Despite of their planar geometry, elliptical dipoles also exhibit nearly omnidirectional dipole-like radiation patterns over a larger than 3 to 1 span in frequency, with a reasonably good directivity level (0–3 dBi). They are linearly polarized, as many of the dipoles employed in commercial systems, but in RDF applications both polarizations can be easily covered by using two different sub-arrays. Elliptically shaped dipole antennas also feature low-dispersion characteristics. In fact, a  $-40$  dB ringing level after twice the duration of the pulse can be achieved together with a stable over DOA phase response [27–29].

The radiating element considered in the proposed design is an elliptical dipole with minor radius 95 mm, eccentricity 1.4, and gap between the antenna flairs equal to 2 mm. The antenna geometry has been optimized in such a way as to obtain a lowest operating frequency  $f \simeq 300$  MHz. To this end, a specific parameter study, not discussed here for sake of brevity, has been carried out by means of the full-wave commercial field solver CST Microwave Studio.

### A) Impact of the curvature radius

Since the considered RDF is basically a circular array, the antenna should be bended over a cylindrical surface. As it is shown in Fig. 1, two possible configurations relevant to the vertical and horizontal polarization of the antenna may be considered.

The curvature radius of the adopted cylindrical substrate ranges from 15 to 45 cm. Figure 2 shows the impact of the curvature radius on the antenna return loss. In order to achieve a physical insight in the antenna characteristics, it is to be noticed that the wideband behavior of the considered radiating element results from the superposition of different modes [30]. The dominant mode is directly linked to the reflection of the surface currents at the open ends of the antenna flairs. Hence, the relevant radiation pattern is similar to that of a conventional linear dipole. At intermediate frequencies the current

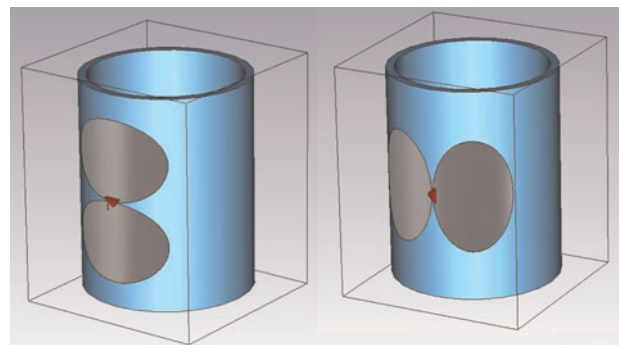


Fig. 1. Two different bending configurations of the butterfly antenna printed over a cylindrical conformal substrate for (a) vertical and (b) horizontal polarization of the radiated field.

distribution is strongly affected by the envelope of the dipole flairs, and the antenna is mainly radiating in the direction of the envelope humps. Finally, at higher frequencies, the modes excited along the dipole arms feature a traveling-wave behavior, so that the radiating element may be regarded as the combination of two opposite tapered slot-line antennas [27]. As it is shown in Fig. 2, bending the antenna along the  $H$ -plane has no impact on the resonant dominant mode and, hence, on the antenna operation at low frequencies. However, a degradation of the antenna response can be noticed at higher frequencies due to the curvature effect of the flair edges. Inversely, when the antenna is bent along the  $E$ -plane, the first resonant mode is strongly affected, whereas the antenna performance is almost the same at higher frequencies.

The conformal deformation of the antenna substrate also has an impact on the radiation properties of the structure. It has been found that reducing the curvature radius results in a larger beamwidth in the  $E$ -plane where the antenna is bent along the  $E$ -plane. Moreover, the front-to-back radiation ratio tends to reduce as the curvature radius decreases (see Fig. 3). Both these effects are in agreement with the physical intuition, taking into account the analogy with the electromagnetic field focusing property of reflector-like antennas.

In conclusion, the antenna bending in the  $H$ -plane is to be preferred since the circuital and radiation characteristics of the structure are less negatively affected by the curvature radius.

## B) Antenna cover

As mentioned in the Introduction, a dielectric radome is needed to protect the RDF sensors against environmental hazards and mechanical impact.

Such cover may be also adopted to enhance the radiation properties of the individual antenna element, increasing the gain and reducing the front-to-back radiation ratio. In this way, the parasitic mutual coupling between the antenna elements and the support structure of the array can be reduced, and the accuracy of the DOA estimation enhanced.

As shown in Fig. 4, the considered antenna element is provided with a high-permittivity dielectric superstrate. It is well-known that the electromagnetic field tends to concentrate in high-dielectric-constant regions, so this layer can stimulate the radiation in the frontward direction enhancing the front-to-back radiation ratio (see Fig. 5). In particular, the antenna response is shifted toward lower frequencies where

the superstrate is used, and the overall return-loss level is improved despite of the appearance of some parasitic resonances (see Fig. 6). Unfortunately, as it can be noticed in Fig. 7, the superstrate is also responsible for a reduction of the antenna bandwidth in terms of absolute gain.

In spite of this, the characteristics of the radiating structure can be enhanced by adding a parallel dielectric layer separated from the superstrate resulting in a combined superstrateradome structure. Such structure is responsible for multiple near-field reflections and interference processes, which can be tuned in order to achieve a better antenna performance in terms of gain and front-to-back radiation ratio. To this end, an extensive parameter study, aimed to the optimization of the superstrate-radome geometry, has been carried out. In this way, it has been found that, where the separation between the dielectric layers is reduced, the antenna response in terms of front-to-back radiation ratio tends to shift toward higher frequencies and, at the same time, the operational bandwidth with respect to the absolute gain level becomes smaller (see Fig. 8). On the other hand, as shown in Fig. 9, by increasing the thickness of the radome, an enhancement in terms of gain and front-to-back radiation ratio can be readily achieved.

## C) Antenna optimization

A specific study has been performed to optimize the geometry of the considered elliptically shaped dipoles. As the individual radiating element is not capable to cover the whole required frequency band, two different antennas have been consequently designed, one to be embedded in a sub-array covering the frequency range from 250 to 950 MHz and the other one for a second sub-array covering the band from 900 MHz to 3.3 GHz. The optimal antenna dimensions are gathered together in Table 1.

The frequency-domain behavior of the return loss featured by the proposed antennas is shown in Fig. 10. Both antennas are characterized by a good impedance matching over the whole operational frequency range. Figures 11 and 12 show the gain and front-to-back radiation ratio of the considered antennas as a function of frequency. As it appears, the gain is greater than 0 dB in the frequency band between 250 and 900 MHz for the first sub-array element, and from 900 MHz to 3 GHz for the second sub-array element. Furthermore, the low- and high-frequency operating antennas feature a front-to-back radiation ratio larger than 0 dB in the relevant operational bands with a peak value of 9 and 8 dB, respectively.

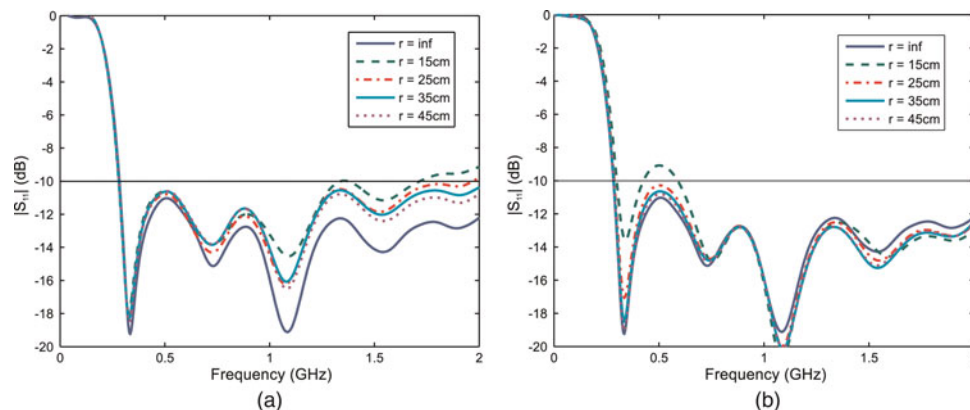


Fig. 2. Frequency behavior of the antenna return loss of the butterfly antenna bent along the  $H$ -plane (a) and  $E$ -plane (b). Planar antenna and curvature radius ranging from 15 to 45 cm.

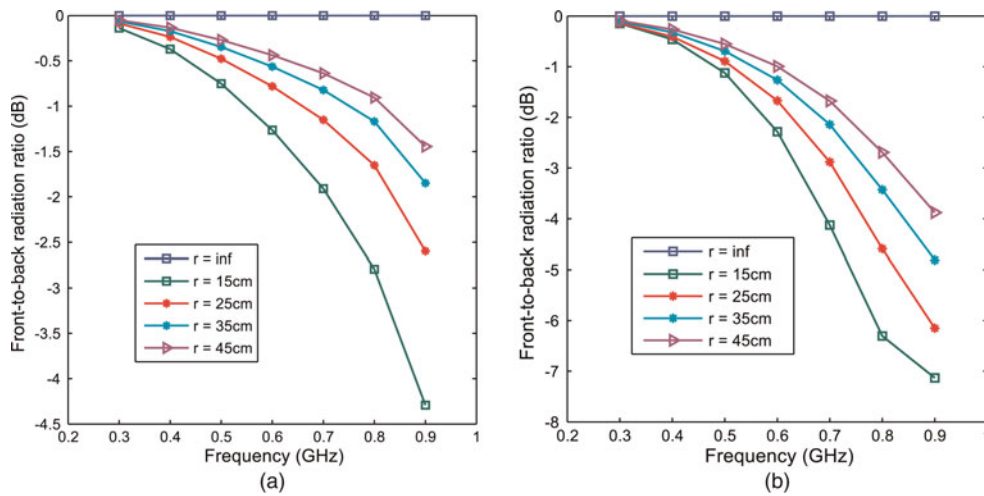


Fig. 3. Frequency domain behavior of the front to back radiation ratio return loss of the butterfly antenna bent along the *H*-plane (a) and *E*-plane (b). Planar antenna and curvature radius ranging from 15 to 45 cm.

The radiation patterns in the *E*- and *H*-plane of the proposed antennas are shown in Figs 13 and 14. As it can be noticed, both antennas are characterized by a donut-like radiation pattern at the lowest frequencies of operation. As the frequency increases the radiated field tends to focus in the frontward direction, resulting in enhanced front-to-back radiation ratio and directivity levels. Finally, at higher frequencies secondary lobes appear, and the field radiation is mainly concentrated along the  $\theta = \pm 90$  directions.

### III. ARRAY DESIGN

It is known that the resolution and accuracy of the estimation increases with the array aperture and the probability of ambiguity decreases with the number of sensors [31].

As it has been shown in Section II, the larger the array radius the better the individual element antenna

performance. Furthermore, the larger the array aperture, the smaller the negative effect of the antenna mutual coupling and errors in the sensor characteristics. So, the selection of the largest possible array radius is a logical choice. Taking this into account, the array radius can be determined according to the size constraints (the maximal radius of 45 and 13cm for the low- and high-frequency operating sub-arrays, respectively).

The minimal number of sensors in each array can be set initially to 5 to avoid the “rank-1” ambiguities [14]. Although the results introduced in [14] assume isotropic radiation patterns and the presented antennas perform a good front-to-back radiation pattern, a more directive radiation pattern reduces the probability of ambiguity, since not only the received phase must be equal, but the magnitude must also be compensated to produce an ambiguous arrival. Therefore, results introduced in [14] can be considered as a worst case for the array design. Further increase of the number of sensors is limited by two considerations:

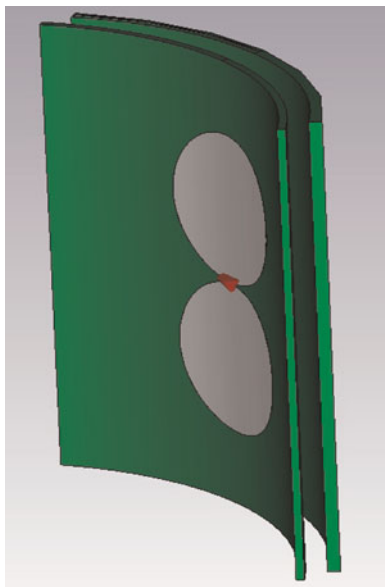


Fig. 4. Sketch of the proposed antenna geometry.

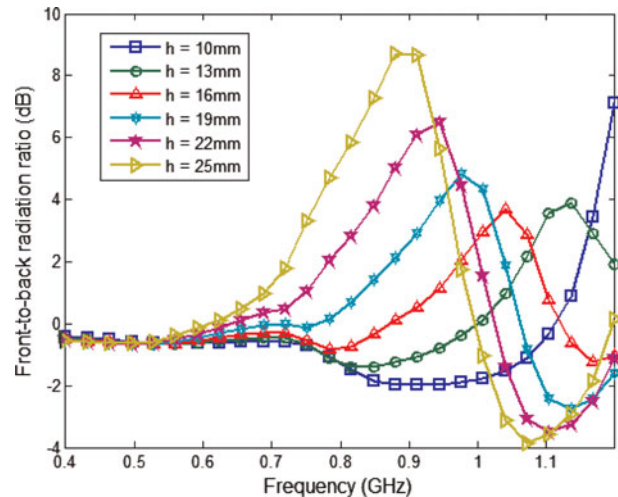


Fig. 5. Frequency-domain behavior of the antenna front-to-back radiation ratio of the conformal butterfly antenna as a function of the superstrate thickness, *h*. The radiating structure is characterized by minor ratio equals 95 mm, eccentricity 1.4, gap between de antenna flairs 2 mm, and curvature radius 45 cm. The superstrate layer has a dielectric constant of 3.5.



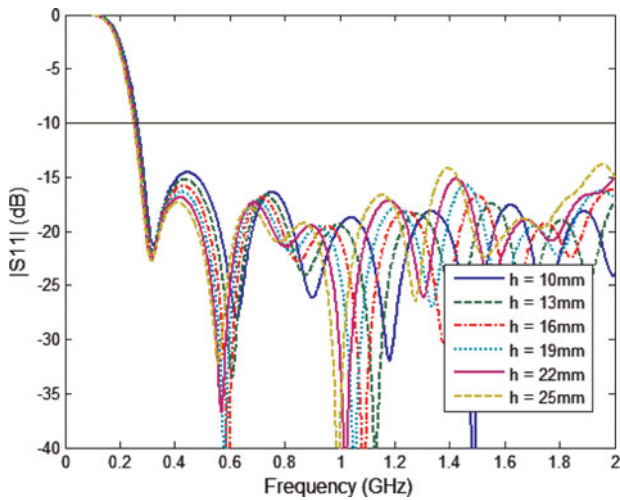


Fig. 6. Frequency-domain behavior of the antenna return loss of the conformal butterfly antenna as a function of the superstrate thickness,  $h$ . The radiating structure is characterized by minor ratio equals 95 mm, eccentricity 1.4, gap between de antenna flairs 2 mm, and curvature radius 45 cm. The superstrate layer has a dielectric constant of 3.5.

- dense arrays have unacceptable high levels of parasitic coupling;
- unnecessary large array apertures should be avoided in order to reduce the probability of ambiguity [15].

Based on the above-mentioned considerations, the selected number of antennas, array radius, and array aperture of the designed arrays have been gathered together in Table 2. In Section V it will be shown that the selected parameters allow meeting the specified design requirements for the RDF.

#### IV. ARRAY CALIBRATION

The mutual coupling between the antenna elements and the effect of the support structure are responsible for a

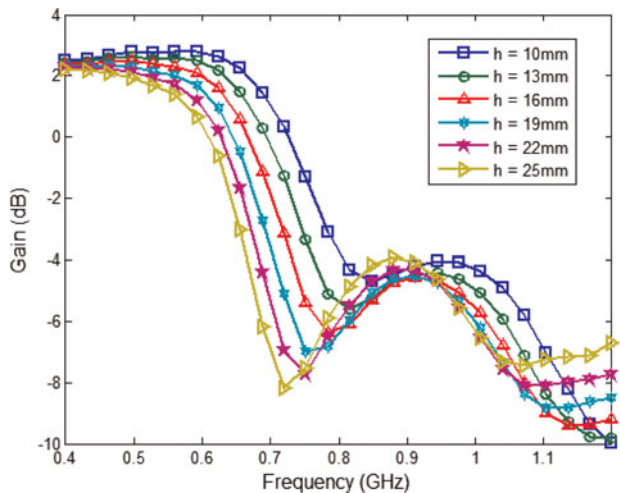


Fig. 7. Frequency-domain behavior of the antenna gain of the conformal butterfly antenna as a function of the superstrate thickness,  $h$ . The radiating structure is characterized by minor ratio equals 95 mm, eccentricity 1.4, gap between de antenna flairs 2 mm, and curvature radius 45 cm. The superstrate layer has a dielectric constant of 3.5.

degradation of the array performance that decreases dramatically the accuracy of the DOA estimation [16–18].

The parasitic antenna coupling can be conveniently evaluated by means of the full-wave analysis of the complete array structure. In particular, Fig. 15 shows the frequency-domain behavior of the return-loss and coupling coefficients between the antenna elements of the low-frequency operating UCA with radius equals to 45 cm. The geometry of the conformal butterfly antenna is defined by the first column of Table 1, whereas the array support structure has been modeled by an infinitely long cylindrical metallic mast with diameter of 7 cm. As it can be noted in Fig. 15, the parasitic coupling between the array elements is relatively high because of the nearly omnidirectional radiation property of the antennas and the reduced inter-element separation.

As for the variations in the antenna characteristics, in the most general case these are related to the following antenna characteristics: gain/phase, position, orientation, and radiation pattern. In general, the radiation pattern of each antenna element can be measured, so errors relevant to the antenna orientation and radiation properties can be readily filtered out. Antenna arrays for RDF applications are usually built in a very accurate manner, and errors in antenna positions are typically negligible. Therefore, only the errors in antenna gain/phase response are accounted in this paper.

It can be easily shown that variations in the antenna characteristics may be conveniently modeled by multiplication of each component of the steering vectors by a complex constant. Since variations in the antenna gain/phase are angle independent, they can be described by a global calibration matrix  $Z$ . However, the calibration method introduced here can be extended by using a local calibration matrix  $Z = Z(\theta)$  to account for possible angle-dependent errors due to the antenna position, orientation, and radiation pattern.

Deterministic calibration methods are usually preferred for an initial calibration. Therefore, attention has been devoted to the development of a suitable deterministic method. In general, a calibration process based on a deterministic method follows three steps. Firstly, a calibration matrix,  $\tilde{A}$ , is defined to model the effect of parasitic coupling and variations in the antenna characteristics. Typically, a complex coupling matrix,  $Z$ , multiplying the ideal steering matrix,  $A$ , is introduced:

$$\tilde{A} = Z \cdot A, \tag{1}$$

where each column of the matrix  $A$  is a steering vector,  $a(\theta_n)$ , which represents the theoretical response of the array in the angular direction,  $\theta_n$ . For example, for a UCA of radius  $R$  and consisting of  $M$  elements, it follows that

$$a(\theta_n) = [a_1(\theta_n) \dots a_m(\theta_n) \dots a_M(\theta_n)]^T, \tag{2}$$

where

$$a_m(\theta_n) = g_m(\theta_n) \exp(jkR \cos[\theta_n - 2(m - 1)\pi/M]), \tag{3}$$

$g_m(\theta_n)$  denoting the response of the  $m$ th antenna in the  $\theta_n$  direction.

Secondly, the steering vectors are measured by using suitable pilot signals and gathered together in the measured

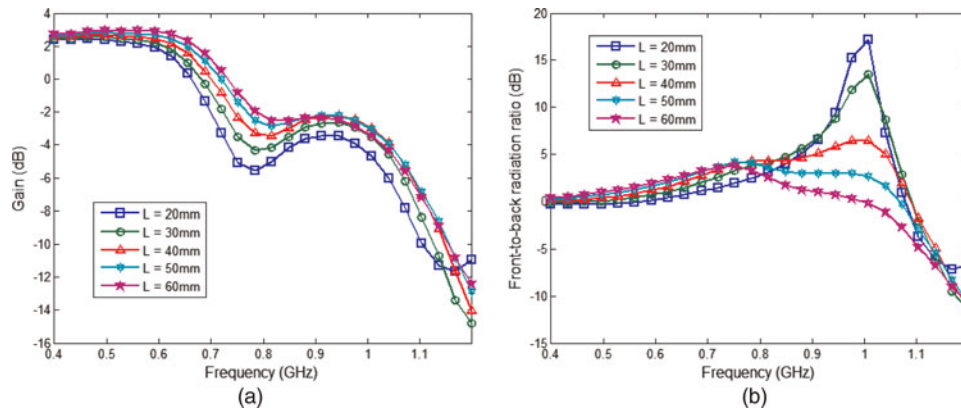


Fig. 8. Frequency-domain behavior of the antenna gain (a) and front-to-back radiation ratio (b) of the conformal butterfly antenna as function of the distance  $L$  between the superstrate and the radome. The radiating structure is characterized by minor ratio equals 95 mm, eccentricity 1.4, gap between the antenna flairs 2 mm, and curvature radius 45 cm. Both the superstrate and the radome have thickness equals 10 mm and relative dielectric constant 3.5.

steering matrix,  $A_m$ . Finally, the mutual coupling matrix,  $Z$ , is estimated via a minimization process in the least squares sense as

$$\hat{Z} = \arg \min_Z \{ \|A_m - \tilde{A}\|^2 \}. \tag{4}$$

The minimization problem is typically solved by adopting a pseudo-inverse-based technique [20]. Additional minimizations are carried out in order to compensate errors in antenna positions [21] or non-idealities in the measurement procedure [22].

A very interesting calibration approach is introduced in [19]. This technique is based on the analytical modeling of the antenna mutual coupling effects. Using this model, it is possible to reduce the number of unknowns in the aforementioned minimization procedure, as well as to take into account the impact of the array support structure.

Unfortunately, the variations in the sensor characteristics are neglected in the calibration approach presented in [19]. Therefore, to overcome this limitation an extended technique is developed in this paper by including the effect of the aforementioned source of error.

Figure 16 shows the different antenna mutual coupling contributions for a five-element UCA. As discussed in [19]

the coupling matrix for this specific array configuration,  $Z_C$ , is a Toeplitz matrix given by

$$Z_C = \begin{bmatrix} 1 & \alpha & \beta & \beta & \alpha \\ \alpha & 1 & \alpha & \beta & \beta \\ \beta & \alpha & 1 & \alpha & \beta \\ \beta & \beta & \alpha & 1 & \alpha \\ \alpha & \beta & \beta & \alpha & 1 \end{bmatrix}, \tag{5}$$

where  $\alpha$  and  $\beta$  denote the coupling coefficients between adjacent and non-adjacent antennas, respectively. Since the variations in the antenna characteristics can be conveniently modeled by the multiplication of each component of the steering vectors by a complex constant, the impact of such non-idealities can be analytically described as the following Hadamard product:

$$\tilde{A} = E \odot A, \tag{6}$$

where the matrix  $E$  is given by

$$E = \begin{bmatrix} e_1 & \dots & e_1 \\ \vdots & \ddots & \vdots \\ e_M & \dots & e_M \end{bmatrix}. \tag{7}$$

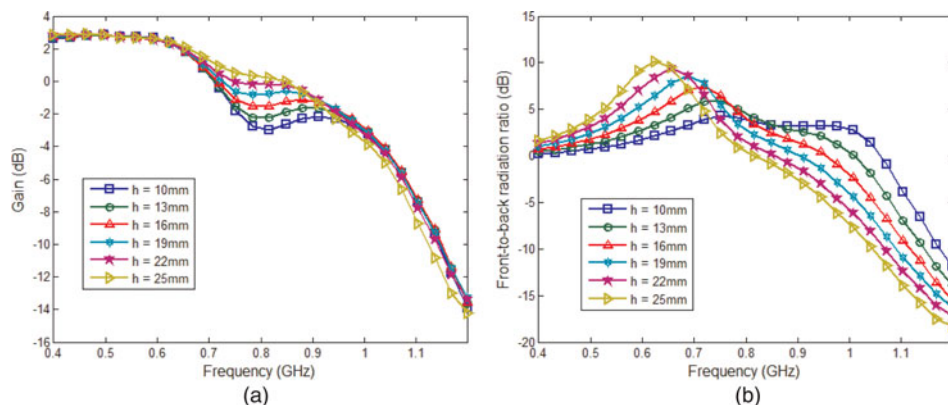


Fig. 9. Frequency-domain behavior of the antenna gain (a) and front-to-back radiation ratio (b) of the conformal butterfly antenna as function of the thickness of the radome layer,  $h$ . The radiating structure is characterized by minor ratio equals 95 mm, eccentricity 1.4, gap between the antenna flairs 2 mm, and curvature radius 45 cm. Both the superstrate and the radome have thickness equals 10 mm and relative dielectric constant 3.5.

Table 1. Antenna optimal dimensions.

Variable	First Subarray	Second Subarray
Radius (mm)	95	27
Eccentricity	1.1	1.1
Gap (mm)	2	1
Superstrate and radome $\epsilon_r$	2.2	2.2
Superstrate height (mm)	10	2.6
Radome height (mm)	16	4.3
Radome separation (mm)	45	12
Curvature radius (cm)	45	13

Furthermore, it is possible to combine both calibration matrices,  $E$  and  $Z_C$ , in the calibration steering matrix:

$$\tilde{A} = Z_C \cdot (E \odot A) = (Z_C \odot M_e) \cdot A = Z_o \cdot A, \tag{8}$$

where  $M_e$  is equal to  $E^T$  reduced to a  $M \times M$  size, and  $Z_o$  is the complete calibration matrix given by

$$Z_o = \begin{bmatrix} e_1 & \alpha e_2 & \beta e_3 & \beta e_4 & \alpha e_5 \\ \alpha e_1 & e_2 & \alpha e_3 & \beta e_4 & \beta e_5 \\ \beta e_1 & \alpha e_2 & e_3 & \alpha e_4 & \beta e_5 \\ \beta e_1 & \beta e_2 & \alpha e_3 & e_4 & \alpha e_5 \\ \alpha e_1 & \beta e_2 & \beta e_3 & \alpha e_4 & e_5 \end{bmatrix}. \tag{9}$$

Additionally, as pointed out in [16], the impact of the array support structure can be usefully modeled by introducing the modified steering vector:

$$\tilde{a}(\theta) = Z \cdot b(\theta) \tag{10}$$

with

$$b = \begin{bmatrix} a(\theta) \\ a_b(\theta) \end{bmatrix}, \tag{11}$$

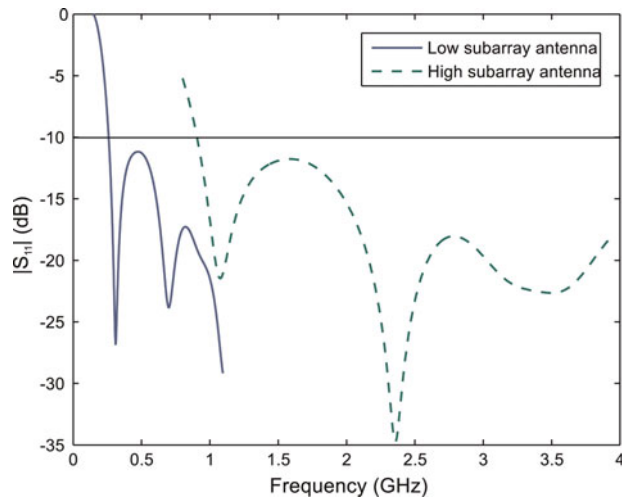


Fig. 10. Frequency-domain behavior of the antenna return loss of the proposed conformal antennas.

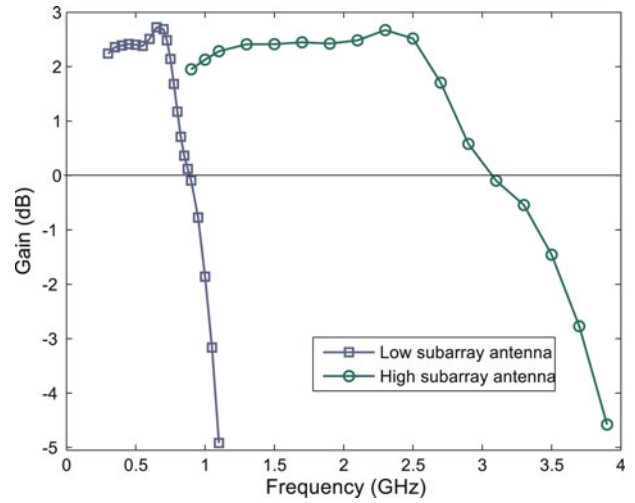


Fig. 11. Frequency-domain behavior of the antenna gain at boresight of the proposed conformal antennas.

$a(\theta)$  being the conventional steering vector, and  $a_b(\theta)$  the steering vector relevant to the support structure and

$$Z = [Z_o Z_b], \tag{12}$$

where

$$Z_b = \begin{bmatrix} \alpha_o & \alpha' & \beta' & \beta' & \alpha' & \gamma \\ \alpha' & \alpha_o & \alpha' & \beta' & \beta' & \gamma \\ \beta' & \alpha' & \alpha_o & \alpha' & \beta' & \gamma \\ \beta' & \beta' & \alpha' & \alpha_o & \alpha' & \gamma \\ \alpha' & \beta' & \beta' & \alpha' & \alpha_o & \gamma \end{bmatrix} \tag{13}$$

is the coupling matrix block accounting for the array mast and the antenna arms. It is worth remarking that this matrix can be extended to effectively describe more complex coupling sources, such as the impact of sub-arrays operating at other frequency bands, or it can be reduced to eliminate sources with low contribution to the coupling. For instance, in a vertically polarized antenna array with low-profile feeding

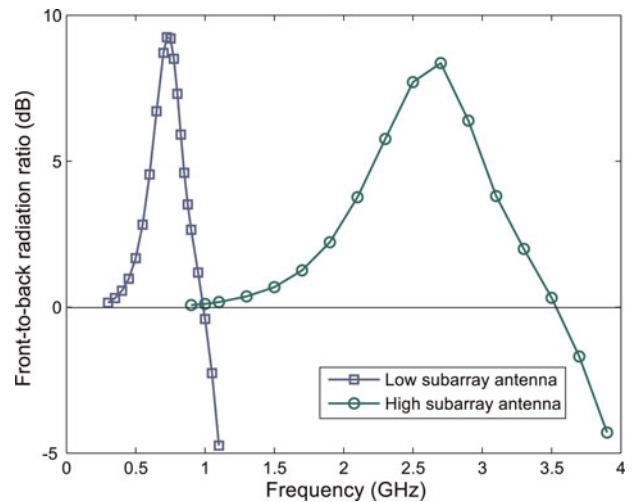


Fig. 12. Frequency-domain behavior of the antenna front-to-back radiation ratio of the proposed conformal antennas.

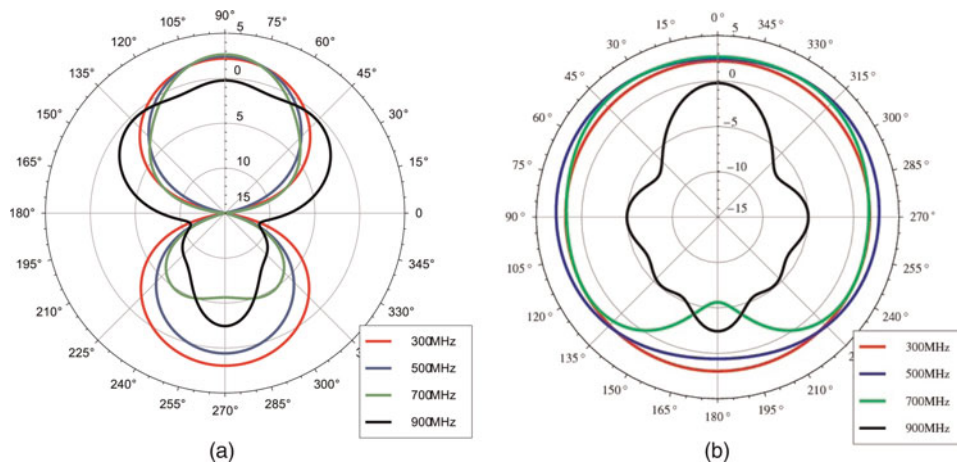


Fig. 13. Antenna gain (dB) of the low-frequency sub-array antenna element along the (a) *E*-plane and (b) *H*-plane.

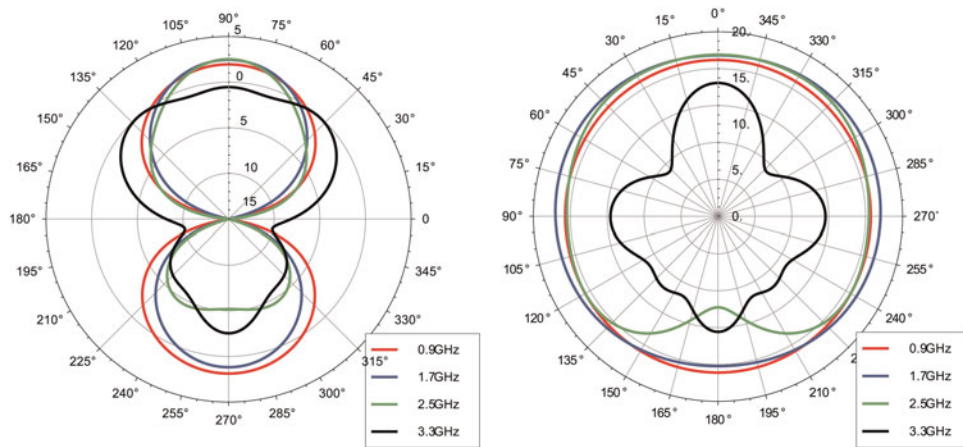


Fig. 14. Antenna gain (dB) of the high-frequency sub-array antenna element along the (a) *E*-plane and (b) *H*-plane.

Table 2. UCA characteristics.

Parameters	First Subarray	Second Subarray
Number of antennas	5	5
Array radius (cm)	45	13
Array aperture (cm)	56.52	16.33

structures the parasitic coupling with the vertically oriented mast is dominant, so we can assume  $\alpha_0 = \beta' = \alpha' = 0$ . In addition, this coupling matrix block can also be extended to properly model variations in the antenna characteristics:

$$Z_b = \begin{bmatrix} e_1 \cdot \gamma \\ e_2 \cdot \gamma \\ e_3 \cdot \gamma \\ e_4 \cdot \gamma \\ e_5 \cdot \gamma \end{bmatrix}. \tag{14}$$

Finally, the minimization of (4) in the least-square sense can be carried out similarly than in [16]. In this way the calibration process is successfully completed.

The proposed calibration technique has been tested with two incoming signals having SNR = 10 dB and separated by

20 impinging on the low-frequency operating UCA consisting of five conformal butterfly antennas whose geometry is described in Table 1. In the considered investigations, the variations in antenna characteristics have been assumed to feature a normal distribution with a 5% standard deviation with respect to the nominal value. Moreover, nine uniformly distributed pilot signals have been employed in the measurement process.

The proposed technique has been compared to the original one [19], and to the conventional calibration technique based on the pseudo-inverse concept [20] (Fig. 17). As it appears from Fig. 17, the performance of the original technique is severely degraded by the presence of variations in antenna characteristics. On the other hand, the performance of the conventional calibration method is degraded due to the effect of the mast. As it can be easily inferred, such degradation is particularly severe at frequencies where the front-to-back radiation ratio of antenna elements is poor.

## V. PERFORMANCE EVALUATION

The performance of the system has been investigated by computing the MSE and the probability of detection (PoD) in different operative scenarios. In this way, one can evaluate



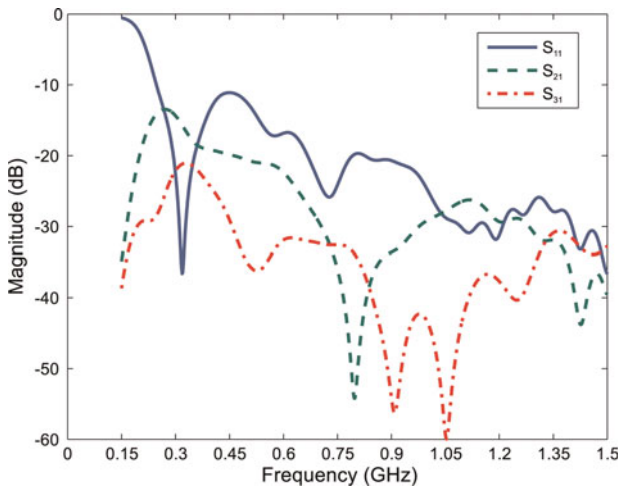


Fig. 15. Return-loss of single antenna element and mutual coupling between antenna elements for a five-element butterfly UCA with array radius equals 45 cm. The supporting structure is modeled by an infinitely long cylindrical metallic mast with diameter 7 cm.

three basic features of the system: the minimum detectable separation between signals; the minimum SNR of operation; and the maximum detectable number of signals. To determine the minimum SNR of operation; the analysis has been carried out by using two well-separated radio signals impinging on the array. The minimum separation between signals is estimated under the assumption of high SNR. Finally, the maximum number of signals is determined by considering well-separated incident radio signals with high SNR. The MUSIC algorithm [32] has been adopted as DOA estimation procedure in order to allow the direct comparison between the designed array and other antenna systems already available in the scientific literature. However, it is to be stressed out that the performance of the whole system can be enhanced by using more advanced algorithms based on the joint estimation of DOA and propagation time of arrival (TOA) [33].

The assessment of the designed RDF has been performed by means of Monte-Carlo simulations with 1000 random selections of the DOA. Figure 17 shows the PoD and MSE for the designed array at different frequencies. No ambiguities

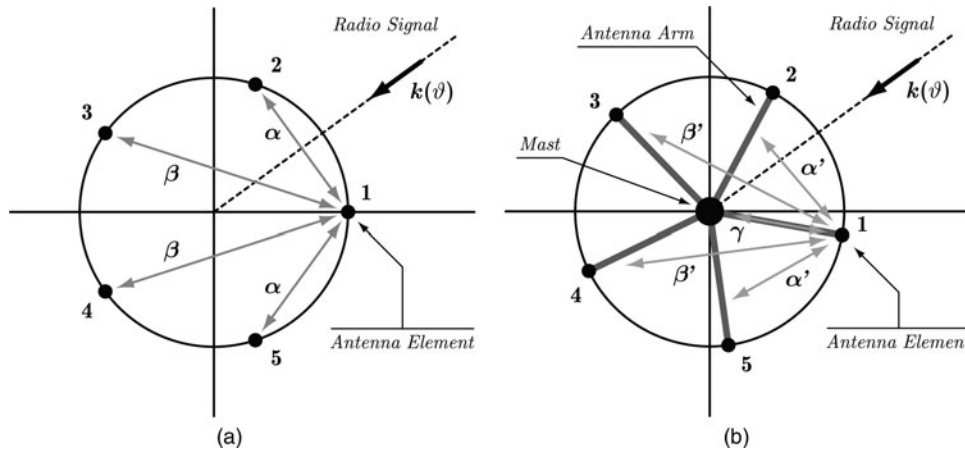


Fig. 16. Parasitic coupling phenomena in an UCA for RDF. Coupling between the array elements (a) and supporting structure (b).

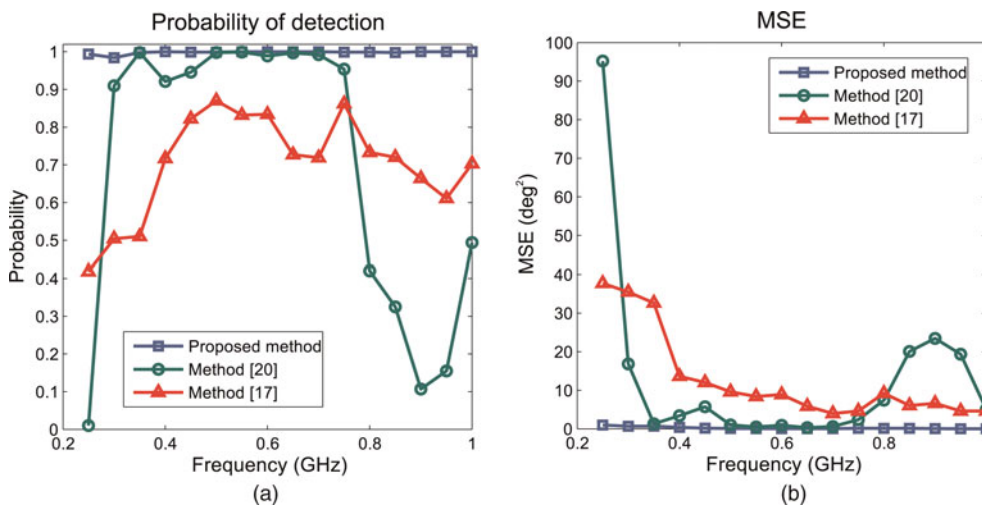


Fig. 17. Probability of detection (a) and MSE (b) for the extended calibration technique and methods introduced in [16, 19], where nine pilot signals have been employed for the calibration. Variations in the antenna characteristics have a normal distribution with a 5% standard deviation of relevant nominal values. Two incoming signals having SNR = 10 dB, and separated by 20° have been employed for the performance evaluation.

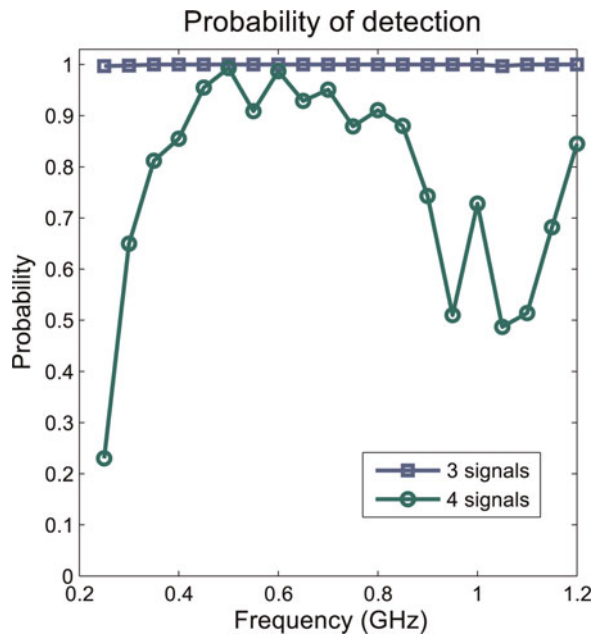


Fig. 18. Probability of detection for a different number of incoming signals with a separation of  $20^\circ$  and SNR equal to 20 dB.

are observed at high frequencies. Theoretically, if  $M$  is the number of sensors, the MUSIC algorithm for DOA estimation is able to detect  $M - 1$  signals [32]. However, where the number of signals approaches the theoretical limit, the system performance starts to degrade (Fig. 18).

The performance of the UCA has been also analyzed for impinging UWB signals. Specific tests have been carried out for two radio signals featuring the same power spectrum (from 150 to 1000 MHz at  $-3$  dB level) and propagating along random spatial directions with a separation of  $20^\circ$ . It has been found that the PoD increases from 87% for SNR =  $-5$  dB up to 100% at SNR = 5 dB, while the MSE decreases from  $6.7 \text{ deg}^2$  (at SNR =  $-5$  dB) to  $4.3 \text{ deg}^2$  (at SNR = 20 dB).

## VI. CONCLUSION

We have designed a compact antenna arrays for RDF system covering the ultra-wide bandwidth from 250 MHz to 3.3 GHz. This design consists in the development of an UWB conformal elliptically shaped dipole array element and antenna radome, as well as in the optimization of the array topology, a novel calibration procedure and assessment of the RDF performance.

An extensive parameter study has been performed in order to investigate the impact of the conformal deformation of the antenna superstrate on the electromagnetic characteristics of the elliptical dipole. An antenna radome has been designed in such a way as to enhance the front-to-back radiation ratio. In order to cover the whole required operational frequency band, two different sub-arrays and antenna elements have been optimized for the [250, 950] MHz and [0.9, 3.3] GHz frequency sub-bands, respectively. As a result, a novel conformal UWB antenna array has been developed. Within its operational sub-bands the optimized antennas are

well matched to the feeding line, featuring frequency-stable donut-like radiation patterns, and reasonably high absolute gain level along the broadside direction. Furthermore, they are characterized by positive front-to-back radiation ratio with a peak value of 8 dB.

As the parasitic mutual coupling between the antenna elements, scattering from the array support structure and variations in the antenna characteristics result in a degradation of the accuracy in the DOA estimation, a novel calibration technique has been developed to compensate for these non-idealities. The main novelty of this calibration technique lies in the fact that it efficiently compensates for performance variations of different antenna elements. Consequently, it outperforms conventional array calibration techniques as it has been shown in simulations. Area of applicability of this technique extends far beyond RDF arrays.

Finally, the performance of the RDF system with the developed antenna arrays has been analyzed by means of Monte-Carlo simulations in different operative scenarios. It has been shown that the RDF guarantees a probability of detection of 0.9 with an MSE smaller than  $50 \text{ deg}^2$  over the whole operation bandwidth. This is fulfilled for a maximum number of signals equals to 3, a minimum separation between signals equals to  $10^\circ$  and a minimum SNR of operation equals to 8 dB. Furthermore, the designed array is free from “rank-1” ambiguities. Although the developed RDF performs similar to existing narrowband systems within their operational bandwidth, it is however capable to efficiently cover the complete radio spectrum from 250 MHz to 3.3 GHz and, in this way, fully satisfy demanding design specifications for future generation RDF applications.

In future research, a dedicated study aimed to the enhancement of the RDF performance in terms of number of detected radio signals (NoS) is to be carried out. To this end, a suitable joint TOA/DOA estimation procedure might be adopted in place of the MUSIC algorithm. This is potentially of great benefit since the limitation on the NoS due to the number of antenna sensors in the RDF can be overcome in this way.

## REFERENCES

- [1] Krim, H.; Viberg, M.: Two decades of array signal processing research. *IEEE Signal Process. Mag.*, **13** (4) (1996), 67–94.
- [2] Russo, M.: Private communications, May 2007.
- [3] Athley, F.; Engdahl, C.; Sunnergren, P.: On radar detection and direction finding using sparse arrays. *IEEE Trans. Aerosp. Electron. Syst.*, **43** (4) (2007), 1319–1333.
- [4] Myungsik, K.; Chong, N.: Direction sensing RFID reader for mobile robot navigation. *IEEE Trans. Autom. Sci. Eng.*, **6** (1) (2009), 44–54.
- [5] Warrington, E.; Stocker, A.; Rizzo, C.: Behaviour of superresolution direction finding algorithms for HF signals propagating through the high latitude ionosphere. *IEE Proc., Microw. Antennas Propag.*, **147** (6) (2000), 469–478.
- [6] Peck, C.; Moore, P.: A direction-finding technique for wide-band impulsive noise source. *IEEE Trans. Vol. Electromagn. Compat.*, **43** (2) (2001), 149–154.
- [7] Tuan, D.; Demmel, F.; Russer, P.: Wideband direction-of-arrival estimation using frequency-domain frequency-invariant beamformers: an analysis of performance. *IEEE Microw. Wirel. Compon. Lett.*, **14** (8) (2004), 383–385.

- [8] Choi, J.; So, J.; Park, C.; Oh, S.: Active composite dipole antenna for direction finding array antenna applications, in *IEEE Antennas Propag. Soc. Int. Symp* 2006.
- [9] Liang, X.; Chia, Y.: New precision wideband direction finding antenna. *IEE Proc., Microw. Antennas Propag.*, **148** (6) (2001), 363–364.
- [10] Hirata, A.: Accuracy compensation in direction finding using patch antenna array with EBG structure. *IEEE Antennas Wirel. Propag. Lett.*, **5** (1) (2006), 1–3.
- [11] Svantesson, T.; Wennstrom, M.: High-resolution direction finding using a switched parasitic antenna, in *Proc. 11th IEEE Signal Processing Workshop on Statistical Signal Processing*, 2001, 508–511.
- [12] Schlub, R.; Thiel, D.: Switched parasitic antenna on a finite ground plane with conductive sleeve. *IEEE Trans. Antennas Propag.*, **52** (5) (2004), 1343–1347.
- [13] Taillefer, E.; Hirata, A.; Ohira, T.: Direction-of-arrival estimation using radiation power pattern with an ESPAR antenna. *IEEE Trans. Antennas Propag.*, **53** (2) (2005), 678–684.
- [14] Xiao, W.; Xiao, X.; Tai, H.: Rank-1 ambiguity DOA estimation of circular array with fewer sensors, in *IEEE The 2002 45th Midwest Symp. on Circuits and Systems*, 2002, MWSCAS-2002.
- [15] Tan, K.; Goh, S.S.; Tan, E.: A study of the rank-ambiguity issues in direction-of-arrival estimation. *IEEE Trans. Signal Process.*, **44** (4) (1996), 880–887.
- [16] Friedlander, B.: A sensitivity analysis of the MUSIC algorithm. *IEEE Trans. Acoust. Speech Signal Process.*, **38** (10) (1990), 1740–1751.
- [17] Friedlander, B.; Weiss, A.J.: Direction finding in the presence of mutual coupling. *IEEE Trans. Antennas Propag.*, **39** (3) (1991), 273–284.
- [18] Ferreol, A.; Larzabal, P.; Viberg, M.: On the asymptotic performance analysis of subspace DOA estimation in the presence of modeling errors: case of MUSIC. *IEEE Trans. Signal Process.*, **54** (3) (2006), 907–920.
- [19] Ferreol, A.; Boyerb, E.; Larzabal, P.; Haardt, M.: On the introduction of an extended coupling matrix for a 2D bearing estimation with an experimental RF system. *Journal of Signal Processing*, **87** (9) (2007), 2005–2016.
- [20] Su, T.; Dandekar, K.; Ling, H.: Simulation of mutual coupling effect in circular arrays for direction-finding applications. *IEEE Microw. Opt. Lett.*, **26** (5) (2000), 331–336.
- [21] Chong Ng, B.; See, C.: Sensor-array calibration using a maximum-likelihood approach. *IEEE Trans. Antennas Propag.*, **44** (6) (1996), 827–835.
- [22] Kortke, A.: A new calibration algorithm for smart antenna arrays, in *The 57th IEEE Semiannual Vehicular Technology Conf. 2003, VTC 2003-Spring*, Vol. 2, April 2003, 1030–1034.
- [23] Lin, M.; Yang, L.: Blind calibration and DOA estimation with uniform circular arrays in the presence of mutual coupling. *IEEE Antennas Wirel. Propag. Lett.*, **5** (1) (2006), 315–318.
- [24] Fieller, A.; Fereol, A.; Larzabal, P.: Robust bearing estimation in the presence of direction-dependent modeling errors: identifiability and treatment, in *IEEE Proc. in Acoustics, Speech, and Signal Processing Int. Conf.*, Detroit, MI, 1995, 1884–1887.
- [25] Jansson, M.; Swindlehurst, A.L.; Ottersten, B.: Weight subspace fitting for general array error models. *IEEE Trans. Signal Process.*, **46** (9) (1998), 284–2498.
- [26] CDF-9200/AVM-3 DF Antenna Datasheet, DRS Technologies.
- [27] Shantz, H.: Planar elliptical element ultra-wideband dipole antennas, in *IEEE APS/URSI Conf.*, 2002.
- [28] Yarovoy, A.G.; Pugliese, R.; Zijderderveld, J.H.; Ligthart, L.P.: Antenna development for UWB impulse radio, in *34th European Microwave Conf.*, 2004, vol. 3, no. 11–15, October 2004, 1257–1260.
- [29] Agrawal, N.; Kumar, G.; Ray, K.: Wide-band planar monopole antennas. *IEEE Trans. Antennas Propag.*, **46** (2) (1998), 294–295.
- [30] Chen, X.; Massey, P.: Operating principles and features of UWB monopoles and dipoles, in *The Institution of Engineering and Technology Seminar on Ultra Wideband Systems, Technologies and Applications*, April 2006, 131–152.
- [31] Baygun, B.; Tamk, Y.: Performance analysis of the MUSIC algorithm in direction finding systems, in *Int. Conf. on Acoustics, Speech, and Signal Processing 1989. ICASSP-89*, vol. 4, no. 23–26, May 1989, 2298–2301.
- [32] Schmidt, R.: Multiple emitter location and signal parameter estimation. *IEEE Trans. Antennas Propag.*, **34** (3) (1986), 276–280.
- [33] VU, V.; Braga, A.; Huyart, B.; Begaud, X.: Joint TOA/DOA measurements for spatio-temporal characteristics of 2.4 GHz indoor Propag. channel, in *The European Conf. on Wireless Technology*, 2005, 47–50.



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